

IN THE UNITED STATES PATENT AND TRADEMARK OFFICE

APPLICATION FOR LETTERS PATENT

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FOR

**Band Reject Filters**

## **BAND REJECT FILTERS**

### **Cross-reference to related application**

- 5 This application is a continuation-in-part application of application serial no. 10/074310 assigned to Nortel Networks Limited.

### **Field of the invention**

- 10 This invention relates to an RF band reject filter, to a base station power amplifier for a cellular radio network, to a duplexer for a mobile telephone handset, and to a low noise amplifier (LNA) input stage.

### **Background of the invention**

- 15 Surface acoustic wave (SAW) devices have been studied and gradually commercialised since the mid 1960s. Such devices typically have electrodes in the form of interlocked "fingers" (so-called inter-digital electrodes) formed on a piezoelectric substrate. When high frequency signals are applied to the input  
20 electrodes, mechanical vibrations in the form of travelling acoustic waves are generated in the piezoelectric substrate which are picked up by the output electrodes. Generally speaking, when the wavelength of the surface acoustic waves and the period of the electrode "fingers" are the same, the magnitude of the surface acoustic waves are at their greatest and the device has a low electrical  
25 impedance. At other input frequencies, the device appears to have a higher electrical impedance.

- Thus, such a so-called "SAW resonator filter" can be made to have a very precise and narrow (typically having a Q factor over 1000), band pass characteristic.  
30 Furthermore, since surface acoustic waves travel across the substrate 100000 times more slowly than the speed of electromagnetic waves, such devices are generally compact. In practice, such devices can be used in a ladder configuration (with a plurality of shunt and plurality of series resonator filters used together). This allows a combined band pass characteristic to be tuned as desired.

Thus such devices have found many uses. However, such devices suffer from two significant disadvantages which prevents their use in some applications. Firstly, band pass filters produced using SAW resonators typically have relatively high insertion losses typically of a minimum of 1 or 2dB. The state of the art presently is an insertion loss of about 1dB in the pass band with a rejection of about 15dB in the stop band for a single stage band pass ladder filter. The losses typically occur as a result of visco-elastic attenuations and/or mode conversions from SAW to bulk acoustic waves when the electrical energy is converted to acoustic energy and travels around the SAW filter cavity. Secondly, the power handling capability of SAW filters is limited. At high powers, the ultrasonic vibration to which the metallic electrodes are subjected eventually causes the metal grain boundaries to migrate. Thus, for example, at the present 1800, 1900 and 2100 MHz cellular mobile bands, such filters cannot be used for a mobile handset duplexer because at these frequencies, such filters cannot survive for a realistic length of time at the desired power levels of approximately 30 dBm.

Relatively little work has been done on SAW notch or band reject filters to date. Of the little work which has been reported, most of it has focussed on the development of narrowband notch filters. One of the first publications on SAW notch filters was in US Patent No. 4,577,168 (Hartman). Various techniques for implementing SAW notch filters are described in which the conductance within the passband of a Single Phase Unidirectional Transducer (SPUDT) SAW transducer was used as an impedance element to create a notch filter. One implementation used the impedance of a SPUDT in conjunction with an RF transformer and other implementations consisted of replacing the capacitors in a bridge -T type notch filter with a SPUDT transducer impedance element. This approach has one disadvantage in that SPUDT transducers fall into the class of Finite Impulse Response Devices and hence the device must be made longer if narrow notch bandwidths are to be achieved. Furthermore, SPUDT type devices are not easily manufactured at elevated frequencies since  $1/8$  wavelength electrodes are required.

A variation of this technique is described in S. Gopani and B.A. Horine "SAW Waveguide-Coupled Resonator Notch Filter", Ultrasonics Symposium, 1990, in which a Two-Pole Waveguide Coupled (WGC) Resonator is embedded in an all pass network to implement a notch filter. This technique has two major

disadvantages. Firstly the WGC resonator is limited to Quartz hence only bandwidth of 0.1 % are attainable and secondly, the resonator has a very poor shape factor of around 5.3 since a typical device might have a 40 dB stopband width of 84 kHz and the 3 dB stopband width of 444 kHz. The device described had a centre frequency of 247 MHz and the insertion losses in the passband were of the order of 4 dB.

A further modification is described in P.A. Lorenz and D.F. Thompson, "Wide Bandwidth Low Cost SAW Notch Filters", Ultrasonics Symposium, 1998. This technique consisted of placing two single pole SAW resonators in series with a resonator in between them. This technique achieved notch depths of more than 40 dB but had a relatively poor shape factor of 4.3 where the 40 dB stopband width was 86 kHz and the 3 dB stopband width was 370 kHz at a centre frequency of 420 MHz. Insertion losses in the stop band were approximately 5 dB or less.

Other simpler implementations consist of using a single pole SAW resonator in series with the signal to obtain a notch at the anti-resonance frequency. Although simple, this filter has a relatively narrow rejection bandwidth, and the shape factor is very poor.

All the reported SAW notch filter developments focused on narrow band notch filters versus wider band reject filters. Furthermore, the techniques consisted of using the impedance of a SAW SPUDT or resonator device in an all pass network to generate a notch response near the passband of the SAW device and leveraged the capacitive properties of the SAW device away from the notch to form an all pass network. Rather poor notch shape factors and insertion losses have been achieved in the reported literature. Therefore there is a need for wider rejection band devices and or lower insertion losses within the passband.

### Summary of the invention

According to a first aspect of the invention there is provided an RF band reject filter comprising a shunt acoustic resonator and a series acoustic resonator, the shunt resonator being arranged to resonate generally at the reject frequency band and the series resonator being arranged to be anti-resonant generally at the reject frequency band.

The precise placement of the series resonator anti-resonance frequency and shunt resonator resonance frequency can be adjusted to achieve a desired tradeoff between rejection band depth or rejection band width as explained in detail below.

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This arrangement overcomes the power handling problem. Conventionally, acoustics resonators are configured to provide a band pass configuration. In this configuration, the series resonators are chosen to be at resonance in the pass band and the shunt resonators are chosen to be at anti-resonance in the pass band.

10 However, by reversing this configuration, a notch or band reject filter is produced.

As factor in achieving very high power handling and very low loss within the pass band is to ensure that the acoustic response is minimal within the pass band. At these frequencies the transducers of the single pole resonators are behaving as  
15 inter-digital capacitors. This is important in achieving very low insertion losses and very high power handling capability at a frequency of interest. The delay through the filter is therefore very short, the power handling capability is thus only be limited by electro-migration or arching across the transducer, which are two mechanisms that occur at much higher power levels than acousto-electric migration. The  
20 insertion loss is also much lower due to the absence of an electric-acoustic-electric conversion and the resulting visco-elastic attenuation and/or mode conversions from SAW to bulk acoustic waves which would result. Thus preferably, the resonators in the filter are arranged to minimise the acoustic response of the filter outside the reject frequency band.

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Such a band reject filter could be used, for example, at a power amplifier output in a base station or handset transceiver with the reject band being tuned to the receive band noise. The filter will readily allow a large transmit signal to pass since the filter is tuned to the receive band and it is thus at receive frequencies that strong acoustic  
30 resonance occurs. Since the receive band power is low, and since in the transmit band there is virtually no acoustic resonance, acoustic-electric migration is not a significant factor in such a filter. Thus, the power handling of such a device in the transmit band is limited by electro-migration (and eventually arcing between the electrodes). This occurs at much higher power levels than the power levels which  
35 may be passed by a prior art band pass acoustic resonator filter at its pass band frequency.

Furthermore, in this band reject configuration of the present invention, the filter appears as a high Q series and shunt capacitor outside its reject band. By including a high Q matching network, the capacitance (outside the reject band) can be substantially reduced so that insertion losses in the region of 0.2dB are attainable for a filter having 15dB attenuation in the reject band.

Thus, for example, such a filter may be used in an UMTS base station in order to reduce the cost of the duplexer module (which presently makes up about 10% of the total cost of the base station cabinet).

As a further enhancement, when SAW band reject filters are used as the resonators, a concatenated structure as described below may be used. The concatenated structure uses a smaller substrate area and also reduces the electrical resistance of the filter relative to an equivalent conventional structure using a plurality of discrete SAW resonators. Thus the overall filter performance may be further improved since the usual trade off in large arrays of SAW resonators between the filter frequency characteristics and the filter loss and also the flexibility of arranging an array of SAW resonators on a substrate, is mitigated.

Thus, in a second aspect, there is provided a base station power amplifier for a cellular radio network, the power amplifier including at least one inter-stage band reject filter comprising a shunt acoustic resonator and a series acoustic resonator, the shunt resonator being arranged to resonate generally at the reject frequency band and the series resonator being arranged to anti-resonant generally at the reject frequency band.

As noted above, for high power applications with low pass-band losses, it is important to ensure that the acoustic response of the filter is minimal within the pass band. At these frequencies the transducers of the single pole resonators are behaving as inter-digital capacitors. This is important in achieving very low insertion losses and very high power handling capability at a frequency of interest. The delay through the filter is therefore very short, the power handling capability is thus only be limited by electro-migration or arching across the transducer, which are two mechanisms that occur at much higher power levels than acousto-electric migration. The insertion loss is also much lower due to the absence of an electric-acoustic-

electric conversion and the resulting visco-elastic attenuation and/or mode conversions from SAW to bulk acoustic waves which would result. Thus preferably, the resonators in the filter are arranged to minimise the acoustic response of the filter outside the reject frequency band.

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The use of the band reject filter of the present invention as an interstage filter for a power amplifier is particularly suitable since as noted above, the band reject filter of the present invention appears as a high Q series and shunt capacitor outside the rejection band. The equivalent capacitor has a short delay and therefore produces a very wideband characteristic with good phase linearity and amplitude flatness. This is in contrast to pass band resonators which have a parabolic group delay and hence poor phase linearity. Furthermore, such pass band resonator filters are (as noted above) too lossy in the pass band and have insufficient amplitude flatness for a cellular radio base station amplifier.

In another aspect, there is provided an LNA input stage including a band reject filter comprising a shunt acoustic resonator and a series acoustic resonator, the shunt resonator being arranged to resonate generally at the reject frequency band and the series resonator being arranged to anti-resonant generally at the reject frequency band. In this configuration, forming part of an LNA input stage, the filter may be used to reject power in the transmit band which is incident on the LNA.

In this way (as explained below), the transmit/receive isolation requirements for the base station duplexer may be reduced, for example, from of the order of 90dB to of the order of 45 dB. This allows a significantly cheaper duplexer to be used for the base station.

Further, another aspect of the invention provides a duplexer for a mobile telephone handset including an RF band reject filter comprising a shunt acoustic resonator and a series acoustic resonator, the shunt resonator being arranged to resonate generally at the reject frequency band and the series resonator being arranged to anti-resonant generally at the reject frequency band.

Such filters may also be used to reject aircraft band interference, TV or radio signals in a handset or base station. They may also be used to suppress an unwanted LO,

sideband or image frequency in a TX or RX chain, where the distortion or loss introduced by a bandpass filter would be unacceptable. Such a situation might arise in the case of a transmitter which must carry a predistorted signal such as would be the case in a system employing a baseband predistortion power amplifier. Since  
5 any filters would be within the correction loop, they must provide very little amplitude or phase distortion over the frequency ranges of interest.

Furthermore, since the equivalent circuit for a SAW resonator and a thin film bulk acoustic resonator (for example, the FBAR product available from Agilent) are  
10 identical, the invention may use a SAW resonator or a thin bulk acoustic resonator for the acoustic resonator component. One advantage of the thin film bulk acoustic resonator implementation is that the filter may be implemented completely in silicon which may, in some applications, provide packaging advantages over a SAW resonator configuration.

15 In a further aspect there is provided a filter comprising a plurality of SAW resonators formed on a common substrate, each SAW resonator sharing an input bus bar or output bus bar with an adjacent SAW resonators in the series, whereby the transducers are electrically equivalent to a discreetly formed group of series-  
20 connected resonators.

In a yet further aspect there is provided a filter comprising a plurality of SAW transducers formed on a common substrate, each SAW transducer being coupled in series with the fingers of one transducer feeding via a transition zone into the fingers  
25 of the next transducer in series the transition zones each being formed as a plurality of nonparallel elongate conductors formed on the substrate and extending between the fingers of each successive transducer in the series, the first and last transducer in series being coupled to an input and output bus bar respectively, whereby the transducers are electrically equivalent to a discreetly formed group of shunt-  
30 connected resonators.

These arrangements provide the concatenated structures mentioned above.

Other aspects and features of the present invention will become apparent to those  
35 ordinarily skilled in the art upon review of the following description of specific embodiments of the invention in conjunction with the accompanying figures.



Brief description of the drawings

5 Figure 1 is a schematic circuit diagram of a ladder configuration of acoustic resonators in accordance with the invention;

Figure 2 is a schematic representation of the circuit of Figure 1 with a high-Q matching network;

10 Figure 3 is a schematic block diagram of a cellular mobile base station including filters in accordance with the invention;

Figure 4 is a schematic diagram of a mobile handset including a duplexer in accordance with the invention;

15 Figure 5 is a plot of simulated S21 parameters for a first embodiment of the filter;

Figure 6 is a plot of simulated S21 parameters for a second embodiment of the filter; and

20 Figure 7 is a plot of simulated S21 parameters for a third embodiment of the filter;

Figure 8 is a schematic representation of an array of series and shunt connected resonators;

25 Figure 9 is a schematic representation of three series connected resonators;

Figure 10 is a plan view of SAW resonators used to implement the resonators of Figure 9;

30 Figure 11 is a plan view of SAW resonators in accordance with the invention which are equivalent to the resonators of Figure 10;

Figure 12 is a schematic representation of three shunt connected resonators;

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- Figure 13 is a plan view of a SAW resonator implementation of the resonators of Figure 12;
- Figure 14 is a plan view of SAW resonator implementation in accordance with the invention, which are equivalent to the resonators of Figure 13;
- Figure 15 is a schematic representation of three series connected resonators;
- Figure 16 is a plan view of a SAW resonator implementation of the schematic representation of Figure 15 using the layout techniques of the invention (Figure 11);
- Figure 17A shows a schematic representation of three series connected resonators connected in parallel;
- Figure 17B shows a circuit equivalent to the circuit of Figure 17A;
- Figure 18 shows a SAW resonator implementation of the schematic circuit of Figure 17B;
- Figure 19 shows the generalised equivalents between a plurality of series connected resonators connected in parallel and a plurality of shunt connected resonators connected in series;
- Figure 21A shows a SAW band reject filter using 1 conventional SAW resonator in parallel;
- Figure 21B shows a narrow reject band SAW filter using a SAW resonator having non-parallel fingers in parallel in accordance with the invention;
- Figure 21C shows a wide reject band SAW filter using a SAW resonator having non-parallel fingers in parallel in accordance with the invention;
- Figure 22 shows an S21 simulated plot of the rejection characteristics of the band reject filters of 21A, 21B and 21C;

Figure 23 is a schematic circuit diagram of two series non-parallel resonators in parallel with an inductance;

5 Figure 24 is a plot showing insertion loss for the circuit of Figure 23;

Figure 25 is a schematic circuit diagram of two shunt non-parallel resonators in parallel with an inductance;

10 Figure 26 is a plot showing insertion loss for the circuit of Figure 25;

Figure 27A shows an array of non-parallel resonators;

Figure 27B shows the array of Figure 8 generalised further and also including resonators having non-parallel resonator fingers;

15 Figure 28 shows a hybrid array of conventional and non-parallel resonators;

Figure 29A shows a layout and corresponding circuit schematic symbol for a convention resonator; and

20 Figure 29B shows a layout and corresponding circuit schematic symbol for a non-parallel resonator.

25 With reference to Figure 1, two series resonators SR2 and SR4 are connected in the series with an input port 6 and an output port 8. Two parallel resonators PR10 and PR12 are connected in a ladder configuration between the series resonators SR4 and SR2 and a ground terminal 14.

30 The resonators may be SAW resonators or thin film bulk acoustic resonators.

The series resonators SR4 and SR2 are designed to present a high impedance at the reject band of interest. This is achieved by designing the filters to be in anti-resonance at the reject band frequency. Shunt or parallel resonators PR10 and PR12 are designed to provide a low impedance at the reject band. This is achieved  
35 by designing these filters to be at or near resonance in the reject band.

Thus, the overall effect of the filter is to provide a high impedance for signals presented between input terminals 6 and 14, at the reject frequency band.

In the applications which are explained in more detail below, one of the desirable characteristics of the filter of Figure 1 is the effect of the filter outside the reject band. In the pass band at frequencies immediately lower than the reject band, the series resonators SR4 and SR2 are at their resonant frequencies while the shunt resonators PR10 and PR12 simply present a capacitive load to ground. In the pass band immediately above the reject band, the shunt resonators PR10 and PR12 are at their anti-resonance frequency and hence present a high impedance to ground while the series resonators SR2 and SR4 present a capacitive series impedance. At frequencies significantly above and below the pass band, the series and shunt resonators simply behave as high Q capacitors.

Thus, in the pass bands either side of the reject band, the filter appears as a high Q series and shunt capacitor. The capacitor has a very short delay in a very wide band characteristic with excellent phase linearity and excellent amplitude flatness. By incorporating high Q matching networks 16 and 17 as shown in Figure 2, the insertion loss of the filter outside the reject band may be reduced to of the order of 0.2dB. The matching networks may be formed as serial and shunt passive inductive and capacitive components as is known in the art.

Optionally, an interstage shunt inductance 19 may be used to aid matching. At frequencies of the order of 2GHz and above, matching may be achieved using microstrip matching.

A symmetric response may be achieved using an optional additional shunt resonator 21.

Although Figures 1 and 2 show a two stage ladder configuration, it will be appreciated that a single stage (or more than two stages) may be used.

Figure 3 shows an application of the type of filter shown in Figures 1 and 2 in a base station for a cellular mobile radio network.

An antenna 20 is used to transmit and receive to and from mobile hand sets at different respective frequencies. A duplexer 22 is used to feed signals in the transmit band, from a power amplifier 24 to the antenna 20 and to feed signals in the receive band from the antenna 20 to a low noise amplifier 26.

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A filter 28 used between amplifier stages 30 and 32 of the power amplifier 24, is used to reject frequencies in the receive band. This reduces the energy present in the receive band at the input 34 to the duplexer.

- 10 Another acoustic resonator band reject filter 36 is tuned to reject the transmit band at the input stage to the low noise amplifier 26.

By incorporating the filters 28 and 36 into the base station design, the duplexer operating margins may be reduced since the sensitivity of the low noise amplifier to energy in the transmit band is reduced by the filter 36 and the likelihood of the power amplifier 24 introducing energy in the receive band into the duplexer 22 is also reduced. Thus the cost of the duplexer 22 may be reduced which will result in a significant cost saving in the overall cost of the base station.

- 20 It will be appreciated that although Figure 3 shows two amplifier stages 30 and 32 and a single interstage filter 28, the number of amplifier stages and the number of interstage filters may vary from that shown. Similarly, the representation of the band reject filter 36 and the single LNA 26 is intended only to represent one possible example of the use of the filter of the present invention.

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Figure 4 shows a mobile telephone handset 40 which incorporates a duplexer which is similar in operation to the duplexer 22 of Figure 3. The purpose of the duplexer is to allow simultaneous transmission and reception in different frequency bands using the same antenna whilst ensuring that relatively high power transmit signals do not swamp the received signals which are to be amplified by the low noise amplifier. As noted above, SAW filters conventionally cannot be used for mobile handset applications in the 1800 MHz or above bands because the combination of high power and relatively high frequency rapidly destroys the filter electrodes. Thus in practice, such duplexers are presently built from ceramic filters. However, since the resonant modes of the filter of the present invention are in the receive band (when used in the transmit circuit segment) the high powers do not damage the filter.

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Thus, both in the base station of Figure 3 and the mobile handset of Figure 4, it is possible to use a SAW filter in the transmit circuit.

5 It will be noted, that the band reject filter may also be used to reject other sources of interference for example from the aircraft band.

The precise placement of the series resonator anti-resonance frequency and shunt resonator resonance frequency can be adjusted to achieve a desired tradeoff between rejection band depth or rejection band width. By placing the frequencies in  
10 close proximity to each other the rejection depth is maximized at the expense of the rejection band width (Figure 5) since the ratio of the series impedance to the shunt impedance is maximized at that frequency. By offsetting the resonance frequency of the shunt resonator slightly above (Figure 6) or slightly below (Figure 7) the anti-resonance frequency of the series resonator, the rejection bandwidth can be  
15 increased at the expense of notch depth.

With reference to Figure 8, the power handling capability of this filter may be increased using arrays of SAW filters 40 and 42. Each array consists of a plurality of series and parallel filters (in the example shown a square array is used  
20 comprising nine filters arranged in a 3 x 3 grid). Assuming that parasitic capacitances are adequately controlled, and assuming that each of the filters in each array is identical, the frequency characteristic of the configuration of Figure 8 is identical to that of a single series and shunt resonator. However, since the voltages and currents across and through each resonator are divided by virtue of the series  
25 and parallel configurations respectively, the overall power handling capability is greatly increased. Thus, for example, using a 3 x 3 array of resonators as shown, the power handling capability is increased by a factor of 9. This may allow the band reject filter to be used at the power amplifier output of a low power (e.g. 5 watt) micro base station, for example. This configuration may be replicated with more  
30 than two arrays.

As a further enhancement to the SAW-implemented embodiments, the shunt and series resonators may be formed using the concatenated structures described below. These structures take up less space on the substrate than the structures  
35 described above which not only provides improved space utilisation in a general

sense but also allows the layout of the type of arrays shown in Figure 8 to be much simplified.

Thus the performance of arrays of the type shown in Figure 8 may be improved since a practical implementation of the array of Figure 8 requires relatively long bus bars (or pads) to connect the transducers to each other which increases the electrical resistance and therefore the loss, of the filter. Accordingly, there is a practical limit on the filter characteristic which may be generated (since for example steep transition band or wide reject band characteristics may require a larger number of resonator elements which in turn reduces the loss performance). By using the concatenated structure as described below, the problems with electrical resistance (and indeed substrate area) are reduced which provides greater design flexibility to produce particular frequency characteristics for the filter or lower loss filters or a combination of the two.

With reference to Figure 9, a schematic representation of three series connected resonators R1, R2, R3 is shown. Figure 10 shows how this arrangement would be implemented using conventional layout designs of resonators R1', R2', R3'.

With reference to Figure 11, the configuration of Figure 10 can instead and in accordance with the invention, be configured so that the output pad of resonator R1'' is shared with the input pad of resonator R2'' to form a shared pad 50. Similarly, a shared pad 52 is formed between resonators R2'' and R3''. It will be appreciated that the substrate area used by the configuration of Figure 11 is much reduced compared to that of Figure 10 but with no degradation of filter performance.

With reference to Figure 12, a schematic representation of shunt connected resonators is shown. In a conventional implementation, the resonators R1', R2' and R3' are implemented using resonators electrically coupled in parallel using electrical coupling lines 54.

Figure 14 shows the superior alternative presented by the invention in which the resonators R1'', R2'' and R3'' are shortened in width and coupled using elongate coupling components 56 which extend between the fingers of the successive resonators. The filter characteristic of the configuration of Figure 14 is the same as that of Figure 13.

Similarly therefore, the arrangement of Figure 14 provides a greatly reduced area of substrate usage providing manufacturing and cost advantages. Furthermore, the noise introduced by the acoustic reflections of adjacent resonators is reduced in this configuration. Effectively rather than three separate interdigital transducers (IDTs) the design is reduced to a single IDT with two reflectors 58. For the conventional layout design shown in Figure 13 the acoustic reflections off the adjacent resonators have significant effects over the overall frequency response of the design.

Figure 15 shows a schematic representation of a three by three array of series connected resonators each connected in parallel as shown by reference numeral 40 in Figure 8. This may be implemented using a parallel array as shown in Figure 16 using three of the filters of Figure 11.

This may be generalised so that any general M by N array of resonators connected as shown in Figure 15 can be implemented in the way shown in Figure 16 with the new type of SAW layout design technique.

Similarly, the array of Figure 17A which is equivalent to the array of Figure 17B, may be implemented with three series connected filters of the type shown in Figure 14 as shown in Figure 18.

This may be generalised as shown in Figure 19 so that any general M by N array of resonators coupled as shown in the upper part of Figure 19 are equivalent to the resonators coupled as shown in the lower part of the figure which may then readily be implemented in the way shown in Figure 18 with the new type of filter configuration.

These may be further generalised in the way shown in Figure 8, in which the arrays 40 or 42 could be any general M by N array of resonators to achieve a desired band reject filter characteristic.

As a yet further enhancement, any of the resonators described above may be replaced with a resonator having non-parallel fingers as shown in Figures 21B and 21C.



Figure 21A shows a conventional SAW resonator for comparison purposes. This non-parallel finger type SAW resonator is particularly advantageous when a relatively wide reject band is desired.

- 5 In the schematic diagrams appended hereto, a non-parallel SAW resonator is shown using the symbol given in Figure 29B. The conventional resonator symbol (and a conventional SAW implementation thereof) is given in Figure 29A for comparison purposes.
- 10 Tapered or non-parallel fingered SAW transducers are described in "Tapered Transducers – Design Applications", Leland Solie, proceedings 1998 IEEE Ultrasonics Symposium, 27-37.

- 15 Figure 22 shows an S21 simulation of the insertion loss of the three filters of Figure 21A, 21B and 21C in a shunt configuration. Respectively, Figure 21A provides a deep and narrow reject band 60, the filter of Figure 21B provides a wider and less deep notch 62 and the wideband configuration of Figure 21C provides a wider and less deep reject characteristic 64.

- 20 The filters of Figures 21B and 21C provide good flexibility since a lower number of this type resonators is required to achieve a desired wide reject band response. . A plurality of the filters may be used together in parallel (Fig.25 and 26) to provide a wide reject band. To achieve the same characteristic using conventional resonators would require a large number of resonators and therefore a large substrate area.
- 25 Thus the use of the non-parallel type resonator shown in Figure 21B or 21C may be used to replace all or part of an array of the type shown in Figure 8 in order to provide a desired band reject characteristic. It will be appreciated that the fingers 66 of the filters of the resonators shown in Figures 21B and 21C need not be straight but could for example have a curving or exponential characteristic. The essential
- 30 characteristic of these filters is that the spacing between the fingers varies through the filter. Generally, the greater the variation, the wider the rejection band.

- Figure 23 is a schematic diagram which demonstrates the characteristic obtained from two non-parallel resonators R1 in series with a matching inductor L. The plot of
- 35 Figure 24 shows the rejection performance of a single one of the resonators R1 and also the rejection performance of the total circuit Rt. It will be noted that by

connecting the resonators in series (with a matching inductance) the overall performance produces a steeper transition band but with worse rejection performance than a filter using single resonator R1.

5 Similarly, Figure 25 shows a schematic diagram of two non-parallel resonators R1 and R3 each having a rejection band generally adjacent in the frequency spectrum and also a matching inductance L. The plot of Figure 26 shows the rejection performance of the filter using single resonator R1 (the rejection performance of R3 is very similar but shifted slightly higher in frequency) and the plot Rt shows the total  
10 performance of the circuit including the matching inductance. It will be noted that this arrangement provides a wider reject band with little performance penalty in terms of transition steepness.

Thus it will be seen that with these building blocks of series and parallel inductors, a  
15 rejection notch of a desired width and transition steepness may be chosen. It will be particularly noted that the configuration shown in Figure 25 provides a wider notch easily. This particular configuration may be expanded in the way shown for example in Figure 27A and Figure 27B. Furthermore, Figure 28 shows that hybrid structures may be used using conventional resonators which may be FBAR or SAW resonators  
20 in conjunction with non-parallel SAW resonators. This provides considerable flexibility in designing band reject filters of the type described above and allows filters to be made to perform in ways that have hitherto not been possible in terms of frequency performance and loss performance.

25 Thus the use of shunt non-parallel SAW resonators as described above means that it is much easier to design a wide band reject filter than using conventional SAW resonators. Also for the same reject band, the design of a band reject filter using the non-parallel SAW resonator is more compact than that using a conventional SAW resonator.

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For the avoidance of doubt, it will be noted that although the invention is described above in connection with single port resonators, multiple port resonators (although believed not to be ideal) could also be used to implement the invention.

35 Thus, in summary, by building a band reject filter using acoustic resonators, it is possible to use SAW resonator filters in applications for which at least the insertion

loss and power handling limitations of conventional band pass resonator filters have proved unsuitable.

5 For the purposes of this specification, the term "RF" and "radio frequency" are to be construed as limited to the range of frequencies within which SAW resonators, FBARs and any equivalent filters may be designed to operate. This is so because the operating frequency of the band reject filter of the present invention is limited only by the capabilities of the resonators from which it is constructed.

10 It will be understood that the band reject filters described above can be designed on a large variety of substrates depending on the application and targeted specifications. It is will be appreciated by those skilled in the art that the term SAW can be extended beyond the classical Rayleigh wave and also encompasses Leaky SAWs, Surface Skimming Bulk Waves and Surface Transverse Waves.

15 The type of wave will depend on the substrate chosen. A few examples of substrates supporting the classical Rayleigh mode are ST Quartz, YZ Lithium Niobate, 128 degree cut X-axis Lithium Niobate, X-cut 112.2 Y-direction Lithium Tantalate, 45X-cut Z-direction Li<sub>2</sub>B<sub>4</sub>O<sub>7</sub> to name a few. Examples of substrates supporting leaky surface acoustic waves are LST Quartz, 64 degree YX Lithium Niobate and 36 to 42 degree YX Lithium Tantalate. Examples of substrates supporting surface skimming bulk waves are Rotated Y-cut ST-quartz, 35.5degree (AT) rotated Y-cut quartz and 36 degree rotated YX-Lithium Tantalate.

25 Furthermore, this device may be designed on multi-layer substrates such as, but not limited to, Lithium Tantalate with an SiO<sub>2</sub> layer or a diamond substrate consisting of Si/Diamond/ZnO/Al/SiO<sub>2</sub> such as that presently being developed by Sumitomo.

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